T-51-09-12

MICRO POWER SYSTEMS

CMOS 12-Bit Monolithic Multiplying DAC

MP7621/7541

FEATURES

- 12-Bit Linearity (0.01%), achieved *without laser trimming* of ladder Rs
- Full Four-Quadrant Multiplication
- .5 ppm/°C Gain Error Tempco
- Plug-In Replacement For AD7541 and AD7521
- TTL/CMOS Compatible
- Low Power Consumption
- Low Feedthrough Error

APPLICATIONS

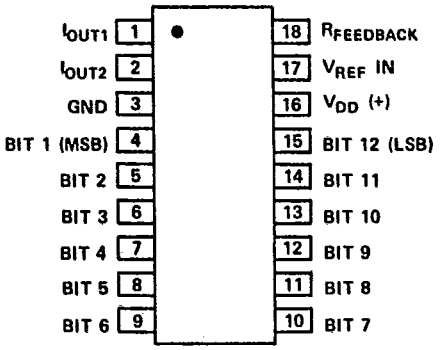
Digital/Synchro Conversion
Programmable Amplifiers
Ratiometric A/D Conversion
Function Generation

GENERAL DESCRIPTION

The MP7621 is a 12-bit monolithic digital-to-analog converter, featuring high-density CMOS. Precision thin-film deposition allows 12-bit linearity without laser trimming, thus eliminating any long-term instabilities the laser might introduce. Thermal compensation reduces Gain Error Tempco to 2 ppm/°C maximum.

Also, the MP7621 is a pin-compatible replacement for Analog Devices' AD7541. It meets or exceeds the performance of that device, with improved supply rejection, improved temperature stability, lower output glitching, and lower variation of linearity and gain error with V_{DD}.

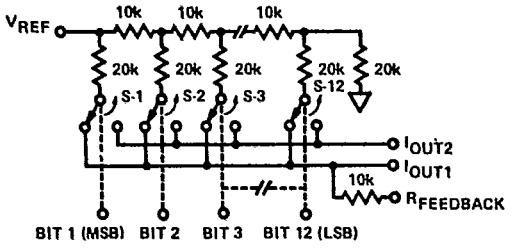
PIN CONFIGURATION



TOP VIEW

See Section 7 for Ordering Information

FUNCTIONAL DIAGRAM



DIGITAL INPUTS (DTL/TTL/CMOS COMPATIBLE)

Logic: A switch is closed to I_{OUT1} for its digital input in a "high" state.

MP7621/7541

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OPERATING TEMPERATURE RANGE UNLESS OTHERWISE NOTED

PARAMETER	7621	7541	TEST CONDITION
STATIC ACCURACY			
Resolution	12 bits min.	12 bits min.	
Nonlinearity			
JN, AD, SD	±0.024% FSR[1] max.	±0.024% FSR max.	$V_{OUT1} = V_{OUT2} = 0V$
KN, BD, TD	±0.012% FSR max.	±0.012% FSR max.	
Nonlinearity Tempco	0.2ppm of FSR/°C max.	0.2ppm of FSR/°C max.	
Gain Error[1,2]	±0.4% FSR max.	±0.4% FSR max.	
Gain Error Tempco[2]	0.5ppm of FSR/°C typ.		
	2ppm of FSR/°C max.	5ppm of FSR/°C max.	
Power Supply Rejection	±.003% per % max.	±0.01% per % max.	V_{DD} = 14.5V – 15.5V 25°C
	±.005% per % max.	±0.02% per % max.	
Output Leakage Current	±50nA max.	±50nA max.	V_{REF} = ±10V 25°C
	±200nA max.	±200nA max.	
DYNAMIC PERFORMANCE			
Output Current Settling Time[3]	1µs max.	1µs max.	To 0.012% of FSR
Feedthrough Error[3]	1mV p-p max.	1mV p-p max.	V_{REF} = 20V p-p @ 10kHz
REFERENCE INPUT			
Input Resistance	5kΩ min., 20kΩ max.	5kΩ min., 20kΩ max.	
DIGITAL INPUTS			
V_{INH}	2.4V min.	2.4V min.	
V_{INL}	0.8V max.	0.8V max.	
Input Leakage Current	±1µA max.	±1µA max.	V_{IN} = 0 or 15V
Input Capacitance[3]	8pF max.	8pF max.	
Input Coding	Binary or Offset Binary (see page 6)		
ANALOG OUTPUTS			
Output Capacitance[3]			
C_{OUT1}	52pF max.	52pF max.	Digital Inputs = V_{INH}
C_{OUT2}	13pF max.	13pF max.	
C_{OUT1}	26pF max.	26pF max.	Digital Inputs = V_{INL}
C_{OUT2}	45pF max.	45pF max.	
POWER REQUIREMENTS			
V_{DD} Range	+5V min., +16V max.	+5V min., +16V max.	Accuracy is guaranteed +10 to +15V, V_{IN}=0.5V
I_{DD}	2mA max.	2mA max.	Digital Inputs: V_{IN}=0.5V

NOTES: [1]FSR is Full Scale Range; [2]Using internal feedback resistor; [3]Guaranteed by design, not subject to test; Specifications subject to change without notice.

ABSOLUTE MAXIMUM RATINGS

(T_A = +25°C unless otherwise noted)

V_{DD} (to GND) . . . . . +17V
V_{REF} (to GND) . . . . . ±25V
Digital Input Voltage Range . . . . . V_{DD} to GND
Output Voltage (Pin 1, Pin 2) . . . . . –300mV to +6.5V
Power Dissipation (Package)
Up to +75°C. 450mW
Derate above +75°C by. . . . . 6mW/°C
Operating Temperature
JN, KN Versions . . . . . 0 to +70°C
AD, BD Versions. . . . . –25°C to +85°C
SD, TD Versions . . . . . –55°C to +125°C
Storage Temperature . . . . . –65°C to +150°C

CAUTION

1. Do not apply voltages higher than V_{DD} or less than GND potential on any terminal except V_{REF}.
2. The digital control inputs are zener protected; however permanent damage may occur on unconnected units under high energy electrostatic fields. Keep unused inputs in conductive foam at all times.

SPECIFICATION DEFINITIONS

NONLINEARITY: Error contributed by deviation of the DAC transfer function from a best straight line function. Normally expressed as a percentage of full scale range. For a multiplying DAC, this should hold true over the entire V_{REF} range.

RESOLUTION: Value of the LSB. For example, a unipolar converter with n bits has a resolution of (2^{-n}) (V_{REF}). A bipolar converter of n bits has a resolution of $[2^{-(n-1)}]$ $[V_{REF}]$. Resolution in no way implies linearity.

SETTLING TIME: Time required for the output function of the DAC to settle to within 1/2 LSB for a given digital input stimulus, i.e., 0 to Full Scale.

GAIN: Ratio of the DAC's operational amplifier output voltage to the input voltage.

FEEDTHROUGH ERROR: Error caused by capacitive coupling from V_{REF} to output with all switches OFF.

OUTPUT CAPACITANCE: Capacity from I_{OUT1} and I_{OUT2} terminals to ground.

OUTPUT LEAKAGE CURRENT: Current which appears on I_{OUT1} terminal with all digital inputs LOW or on I_{OUT2} terminal when all inputs are HIGH.

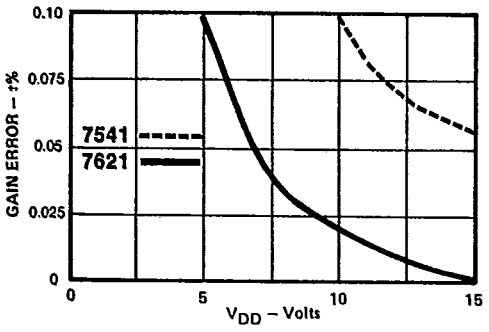


Figure 2. Supply Current vs. Supply Voltage, 7621

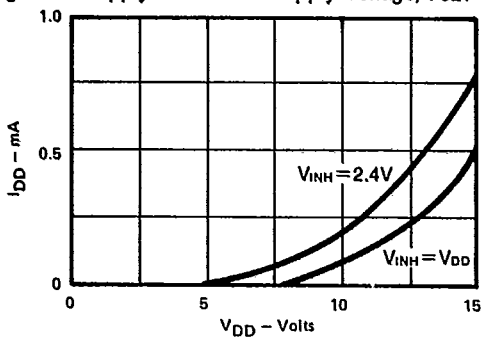


Figure 3. Linearity Error vs. Supply Voltage Typ.

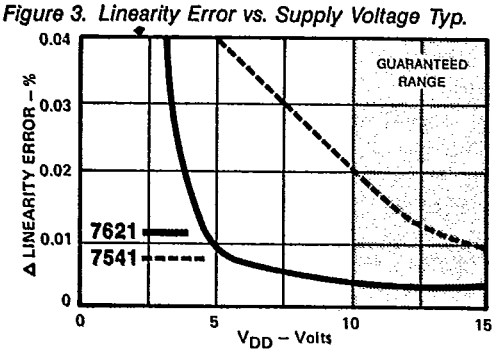
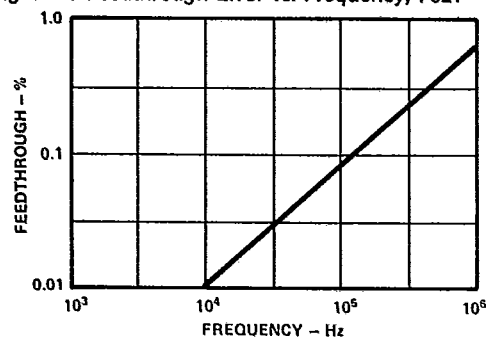


Figure 4. Feedthrough Error vs. Frequency, 7621



APPLICATION HINTS

Linearity depends upon the potential of I_{OUT1} and I_{OUT2} (pin 1 and pin 2) being exactly equal to GND (pin 3) and the output amplifier's non-inverting (+) input. Careful PC board layout and adjustment and selection of the amplifier's offset voltage and bias current are necessary, any resistance in series with I_{OUT2} will degrade linearity at $1\Omega \cong 0.4$ LSB.

The input structures of some high speed operational amplifiers can attempt to draw substantial current during switch-on. Schottky diodes should be used in these circumstances to prevent the absolute maximum rating for V_{OUT1} and V_{OUT2} being exceeded.

The power supply should be carefully checked for noise, which would affect performance, and overshoot which could damage the device.

Unused digital inputs must always be grounded or taken to V_{DD} to ensure correct operation. Particular care should be taken when digital inputs are routed to another PC card. It is recommended that inputs open-circuited when PC cards are disconnected be taken to V_{DD} or GND via high value (1MΩ) resistors to prevent the accumulation of static charges.

CIRCUIT DESCRIPTION

GENERAL CIRCUIT INFORMATION

The MP7621, a 12-bit multiplying D/A converter, consists of a highly stable thin film R-2R ladder and twelve CMOS current switches on a monolithic chip. Most applications require the addition of only an output operational amplifier and a voltage or current reference.

The simplified D/A circuit is shown in Figure 5. An inverted R-2R ladder structure is used– that is, the binarily weighted currents are switched between the I_{OUT1} and I_{OUT2} bus lines thus maintaining a constant current in each ladder leg independent of the switch state.

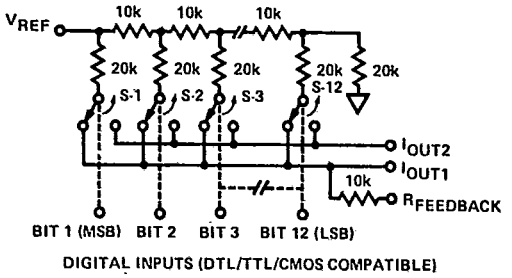
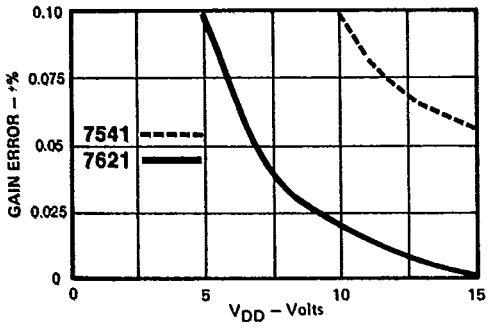


Figure 5. MP7621 Functional Diagram (Inputs "HIGH")

One of the CMOS current switches is shown in Figure 6. The geometries of devices 1, 2 and 3 are optimized to make the digital control inputs DTL/TTL/CMOS compatible over the full military temperature range. The input stage drives two inverters (devices 4, 5, 6 and 7) which in turn drive the two output N-channels. The "ON" resistances of the switches are binarily scaled so the voltage drop across each switch is the same. For example, switch 1 of Figure 5 was designed for an



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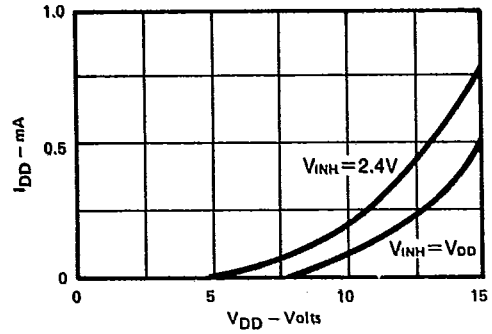

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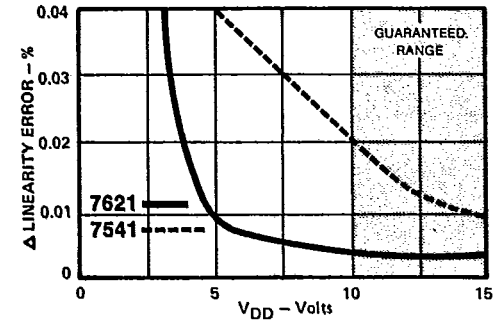

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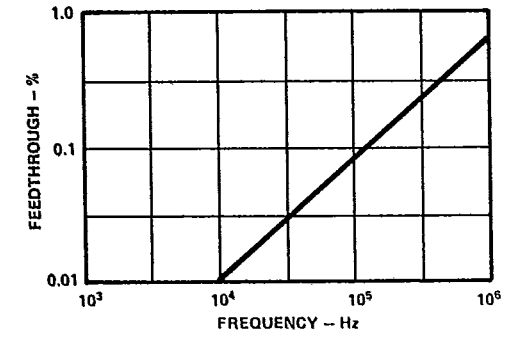

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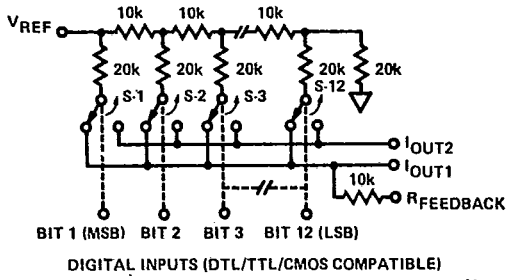

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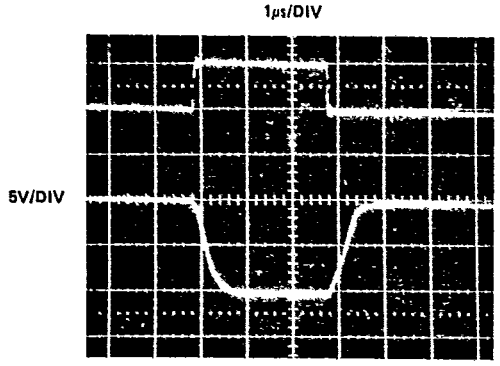

Figure 12. Output Waveform

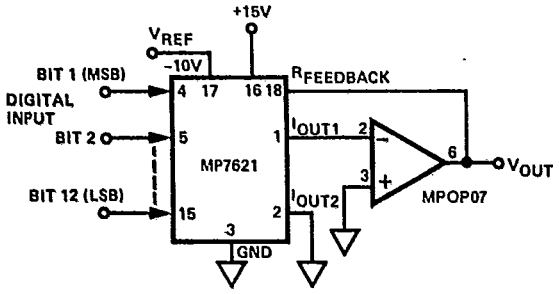

Figure 13. DAC Circuit Using MPOP07

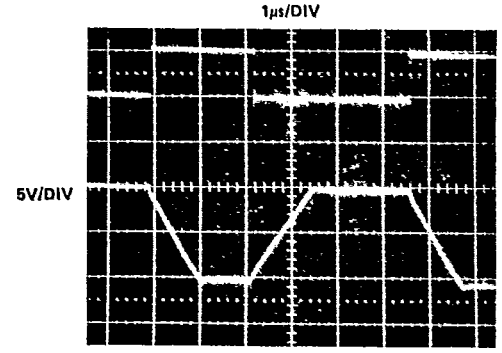

Figure 14. Output Waveform

The circuits and waveforms shown in Figures 9 to 14 are representative of the three types of output amplifiers: a general purpose low drift MPOP02, a high speed low cost MPOP01, and low offset MPOP07.

Points to remember when applying high speed amplifiers include:

1. Protection diodes as shown in Figures 15 and 16.
2. Phase compensation for the DAC's output capacitance.
3. Power supply decoupling and correct load earthing.

APPLICATIONS

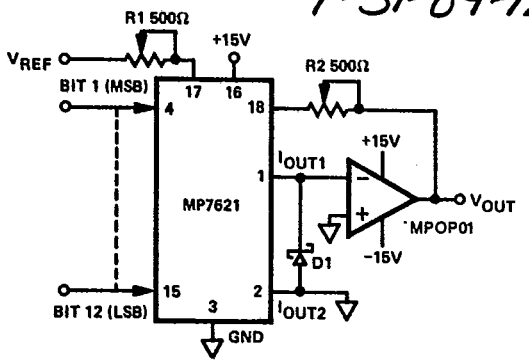

Figure 15. Unipolar Binary Operation

UNIPOLAR BINARY OPERATION

The connections required for unipolar digital binary operation are shown above. V_{REF} may be positive or negative so 2-quadrant multiplication may be performed. Schottky diode D1 prevents I_{OUT1} from negative excursions which could damage the device. This precaution is only necessary with certain high speed amplifiers.

BIPOLAR (4-QUADRANT) BINARY OPERATION

The digital input is offset binary coded and multiplies V_{REF} according to Table 2. Resistors R1 and R2 should be equal within 0.1% at all temperatures, but need not track the resistors within the MP7621. D1 and D2 perform the same function as in Figure 15. Network R3, R4, R5 sum ½LSB of current into I_{OUT2} to ensure correct coding at zero.

R1 or R2 can be adjusted to produce the outputs shown in Table 1. However, it is recommended that when the application permits it R1 and R2 be omitted. The typical gain error in this condition is 0.3% of full scale. The offset voltage of amplifier A1 should be adjusted to less than 0.5mV over the temperature range.

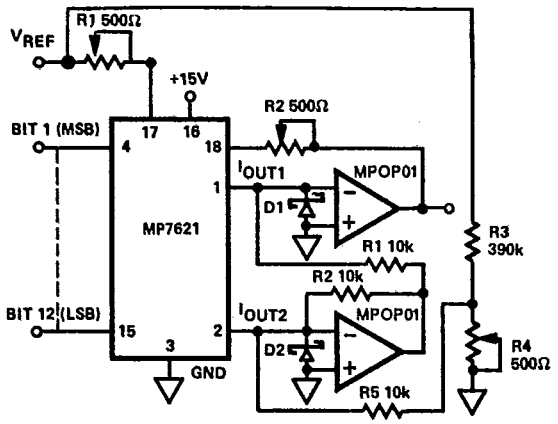

Figure 16. Bipolar (4-Quadrant) Binary Operation

DIGITAL INPUT	NOMINAL ANALOG OUTPUT
111111111111	−0.99975 V_{REF}
100000000000	−0.50000 V_{REF}
010000000000	−0.49975 V_{REF}
000000000000	0

Table 1. Code Table for Circuit of Figure 15.

DIGITAL INPUT	NOMINAL ANALOG OUTPUT
111111111111	−0.99951 V_{REF}
100000000001	−0.00049 V_{REF}
100000000000	0
010000000000	+0.50000 V_{REF}
000000000000	+1.00000 V_{REF}

Table 2. Code Table for Circuit of Figure 16.

Amplifiers A1 and A2 should be adjusted to an input offset of less than 0.1mV and should be better than 0.5mV over the temperature range. With V_{REF} set to approximately 10V, R4 should be adjusted so that with code 100000000000 V_{OUT} = 0V ±0.2mV. R1 or R2 should be adjusted so that with code 000000000000 $V_{OUT} = V_{REF}$.

As with the unipolar circuit R1 and R2 can be omitted, with a resulting typical gain error of 0.3% of full scale. R4 may be replaced by a 100Ω fixed resistor. The typical zero error if this is done is 0.015% of F.S.R.

OUTPUT AMPLIFIER CONSIDERATIONS

It has already been pointed out that the DAC output resistance varies with the digital code. The effect this has on static accuracy will now be considered.

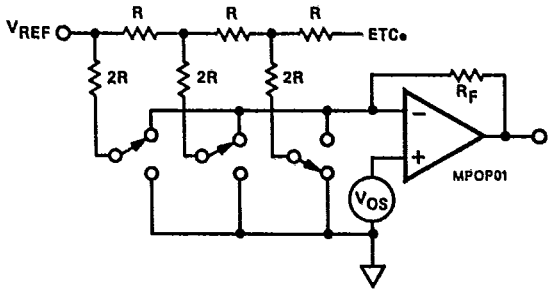

Figure 17.

$$\text{The error voltage} = V_{OS}\left(1+\frac{R_F}{R_O}\right)$$

R_O is a function of the digital code.
$R_O \cong 10k\Omega$ for any more than 4-bits Logic 1.
$R_O \cong 30k\Omega$ for any single bit Logic 1.

The gain for offset, therefore, changes as follows:

$$\text{At code 001111111111 } V_{ERROR1} = V_{OS}\left(1+\frac{10k}{10k}\right) = 2\,V_{OS}$$

$$\text{At code 010000000000 } V_{ERROR2} = V_{OS}\left(1+\frac{10k}{30k}\right) = \frac{4}{3}V_{OS}$$

The error difference is therefore $\frac{2}{3}V_{OS}$.

Since, for a 12-bit resolution DAC, one LSB has a weight (for V_{REF} = +10V) of 2.5mV, it is clearly important that V_{OS} be nulled, either using the amplifier's nulling facility or an external network.

It is important to realize that an offset can be caused by including the usual bias current compensation resistor in the amplifier's non-inverting input terminal. This should not be included. Instead the amplifier should have a bias current which is low over the temperature range of interest, and should certainly not exceed 75nA.

ANALOG/DIGITAL DIVISION

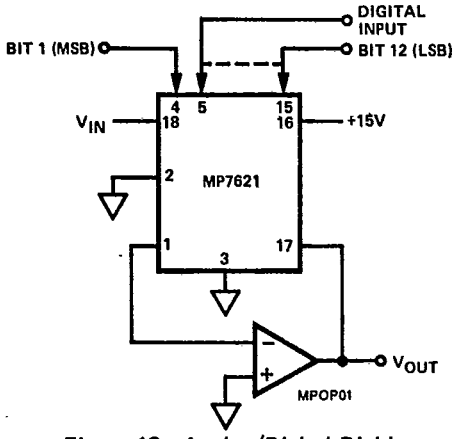

Figure 18. Analog/Digital Divider

With the MP7621 connected in its normal multiplying configuration as shown in Figure 15, the transfer function is

$$V_O = -V_{IN}\left(\frac{A_1}{2^1}+\frac{A_2}{2^2}+\frac{A_3}{2^3}+\cdots\cdots\frac{A_{12}}{A^{12}}\right)$$

where the coefficients A_X assume a value of 1 for an ON bit and 0 for an OFF bit.

By connecting the DAC in the feedback of an operational amplifier, as shown in Figure 18, the transfer function becomes

$$V_O = \left(\frac{-V_{IN}}{\frac{A_1}{2^1}+\frac{A_2}{2^2}+\frac{A_3}{2^3}+\cdots\cdots\frac{A_{12}}{A^{12}}}\right)$$

This is division of an analog variable (V_{IN}) by a digital word. With all bits off, the amplifier saturates to its bound, since division by zero is not defined. With the LSB (Bit 12) ON, the gain is 4096. With all bits ON, the gain is 1 (±1LSB).

DIGITAL/SYNCHRO CONVERTER

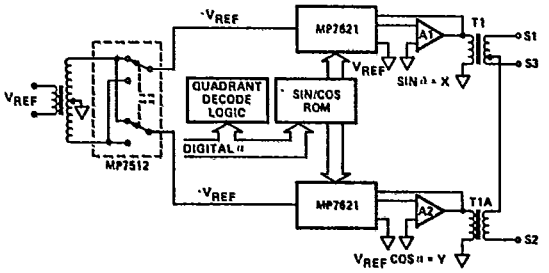

Figure 19. 14-Bit Digital to Synchro Converter

The low cost and high accuracy available from the MP7621, together with its bipolar multiplying capability, are exploited fully in the circuit of Figure 19. V_{REF} is commonly 400Hz but by replacing the transformers with dc-coupled circuits coordinate transformation may be performed.

The SIN/COS ROM is readily available at low cost and the MP7512 switch enables greater resolution to be obtained.

Resolver-to-synchro transformation is performed by the Scott connected pair T1 and T1A. The power available to the load connected to S1, S2 and S3 is determined by the amplifiers A1 and A2. A particular advantage of the circuit shown in Figure 19 is that it is invariant with respect to θ, and may be used to directly drive equipment such as CRT displays.